

FAN7930B

Critical Conduction Mode PFC Controller

Features

- Additional OVP Detection Pin
- Input Voltage Absent Detection Circuit
- Maximum Switching Frequency Limitation
- Internal Soft-Start and Overshoot-less Control
- Internal Total Harmonic Distortion (THD) Optimizer
- Precise Adjustable Output Over-Voltage Protection
- Open-Feedback Protection and Disable Function
- Zero Current Detector
- 150µs Internal Startup Timer
- MOSFET Over-Current Protection
- Under-Voltage Lockout with 3.5V Hysteresis
- Low Startup and Operating Current
- Totem-Pole Output with High State Clamp
- +500/-800mA Peak Gate Drive Current
- 8-Pin Small Outline Package (SOP)

Applications

- Adapter
- Ballast
- LCD TV, CRT TV
- SMPS

Description

The FAN7930B is an active power factor correction (PFC) controller for boost PFC applications that operate in critical conduction mode (CRM). It uses a voltage-mode PWM that compares an internal ramp signal with the error amplifier output to generate a MOSFET turn-off signal. Because the voltage-mode CRM PFC controller does not need rectified AC line voltage information, it saves the power loss of an input voltage sensing network necessary for a current-mode CRM PFC controller.

FAN7930B provides over-voltage protection, open-feedback protection, over-current protection, input-voltage-absent detection, and under-voltage lockout protection. The additional OVP pin can be used to shut down the boost power stage when output voltage exceeds OVP level due to the resistors that are connected at INV pin are damaged. The FAN7930B can be disabled if the INV pin voltage is lower than 0.45V and the operating current decreases to a very low level. Using a new variable on-time control method, THD is lower than the conventional CRM boost PFC ICs.

Related Resources

[AN-8035 — Design Consideration for Boundary Conduction Mode PFC Using FAN7930](#)

Ordering Information

Part Number	Operating Temperature Range	Top Mark	Package	Packing Method
FAN7930BM	-40 to +125°C	FAN7930B	8-Lead Small Outline Package (SOP)	Rail
FAN7930BMX				Tape & Reel

Pin Configuration

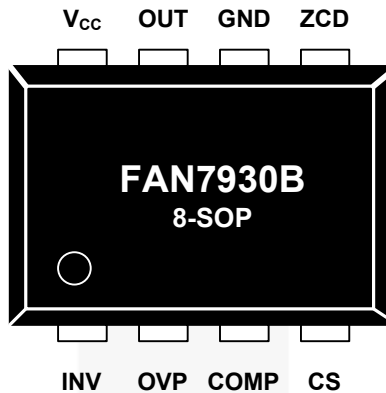


Figure 3. Pin Configuration (Top View)

Pin Definitions

Pin #	Name	Description
1	INV	This pin is the inverting input of the error amplifier. The output voltage of the boost PFC converter should be resistively divided to 2.5V.
2	OVP	This pin is used to detect PFC output over voltage when INV pin information is not correct.
3	COMP	This pin is the output of the transconductance error amplifier. Components for the output voltage compensation should be connected between this pin and GND.
4	CS	This pin is the input of the over-current protection comparator. The MOSFET current is sensed using a sensing resistor and the resulting voltage is applied to this pin. An internal RC filter is included to filter switching noise.
5	ZCD	This pin is the input of the zero-current detection block. If the voltage of this pin goes higher than 1.5V, then goes lower than 1.4V, the MOSFET is turned on.
6	GND	This pin is used for the ground potential of all the pins. For proper operation, the signal ground and the power ground should be separated.
7	OUT	This pin is the gate drive output. The peak sourcing and sinking current levels are +500mA and -800mA, respectively. For proper operation, the stray inductance in the gate driving path must be minimized.
8	V _{CC}	This is the IC supply pin. IC current and MOSFET drive current are supplied using this pin.

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Absolute Maximum Ratings

Stresses exceeding the absolute maximum ratings may damage the device. The device may not function or be operable above the recommended operating conditions and stressing the parts to these levels is not recommended. In addition, extended exposure to stresses above the recommended operating conditions may affect device reliability. The absolute maximum ratings are stress ratings only.

Symbol	Parameter	Min.	Max.	Unit
V_{CC}	Supply Voltage		V_Z	V
I_{OH}, I_{OL}	Peak Drive Output Current	-800	+500	mA
I_{CLAMP}	Driver Output Clamping Diodes $V_O > V_{CC}$ or $V_O < -0.3V$	-10	+10	mA
I_{DET}	Detector Clamping Diodes	-10	+10	mA
V_{IN}	Error Amplifier Input, Output, OVP Input, ZCD and OVP Pin ⁽¹⁾	-0.3	8.0	V
	CS Input Voltage ⁽²⁾	-10	6	
T_J	Operating Junction Temperature		+150	°C
T_A	Operating Temperature Range	-40	+125	°C
T_{STG}	Storage Temperature Range	-65	+150	°C
ESD	Electrostatic Discharge Capability	Human Body Model, JESD22-A114	2.5	kV
		Charged Device Model, JESD22-C101	2.0	

Notes:

- When this pin is supplied by external power sources by accident, its maximum allowable current is 50mA.
- In case of DC input, acceptable input range is -0.3V~6V: within 100ns -10V~6V is acceptable, but electrical specifications are not guaranteed during such a short time.

Thermal Impedance

Symbol	Parameter	Min.	Max.	Unit
Θ_{JA}	Thermal Resistance, Junction-to-Ambient ⁽³⁾	150		°C/W

Note:

- Regarding the test environment and PCB type, please refer to JESD51-2 and JESD51-10.

Electrical Characteristics

$V_{CC} = 14V$, $T_A = -40^{\circ}C \sim +125^{\circ}C$, unless otherwise specified.

Symbol	Parameter	Conditions	Min.	Typ.	Max.	Units
V_{CC} Section						
V_{START}	Start Threshold Voltage	V_{CC} Increasing	11	12	13	V
V_{STOP}	Stop Threshold Voltage	V_{CC} Decreasing	7.5	8.5	9.5	V
HY_{UVLO}	UVLO Hysteresis		3.0	3.5	4.0	V
V_Z	Zener Voltage	$I_{CC}=20mA$	20	22	24	V
V_{OP}	Recommended Operating Range		13		20	V
Supply Current Section						
I_{START}	Startup Supply Current	$V_{CC}=V_{START}-0.2V$		120	190	μA
I_{OP}	Operating Supply Current	Output Not Switching		1.5	3.0	mA
I_{DOP}	Dynamic Operating Supply Current	50kHz, $C_I=1nF$		2.5	4.0	mA
I_{OPDIS}	Operating Current at Disable	$V_{INV}=0V$	90	160	230	μA
Error Amplifier Section						
V_{REF1}	Voltage Feedback Input Threshold1	$T_A=25^{\circ}C$	2.465	2.500	2.535	V
ΔV_{REF1}	Line Regulation	$V_{CC}=14V \sim 20V$		0.1	10.0	mV
ΔV_{REF2}	Temperature Stability of $V_{REF1}^{(4)}$			20		mV
$I_{EA,BS}$	Input Bias Current	$V_{INV}=1V \sim 4V$	-0.5		0.5	μA
$I_{EAS,SR}$	Output Source Current	$V_{INV}=V_{REF}-0.1V$		-12		μA
$I_{EAS,SK}$	Output Sink Current	$V_{INV}=V_{REF}+0.1V$		12		μA
V_{EAH}	Output Upper Clamp Voltage	$V_{INV}=1V$, $V_{CS}=0V$	6.0	6.5	7.0	V
V_{EAZ}	Zero Duty Cycle Output Voltage		0.9	1.0	1.1	V
g_m	Transconductance ⁽⁴⁾		90	115	140	μmho
Maximum On-Time Section						
$t_{ON,MAX1}$	Maximum On-Time Programming 1	$T_A=25^{\circ}C$, $V_{ZCD}=1V$	35.5	41.5	47.5	μs
$t_{ON,MAX2}$	Maximum On-Time Programming 2	$T_A=25^{\circ}C$, $I_{ZCD}=0.469mA$	11.2	13.0	14.8	μs
Current-Sense Section						
V_{CS}	Current Sense Input Threshold Voltage Limit		0.7	0.8	0.9	V
$I_{CS,BS}$	Input Bias Current	$V_{CS}=0V \sim 1V$	-1.0	-0.1	1.0	μA
$t_{CS,D}$	Current Sense Delay to Output ⁽⁴⁾	$dV/dt=1V/100ns$, from 0V to 5V		350	500	ns

Continued on the following page...

Electrical Characteristics

$V_{CC} = 14V$, $T_A = -40^{\circ}C \sim +125^{\circ}C$, unless otherwise specified.

Symbol	Parameter	Conditions	Min.	Typ.	Max.	Units
Zero-Current Detect Section						
V_{ZCD}	Input Voltage Threshold ⁽⁴⁾		1.35	1.50	1.65	V
HY_{ZCD}	Detect Hysteresis ⁽⁴⁾		0.05	0.10	0.15	V
V_{CLAMPH}	Input High Clamp Voltage	$I_{DET}=3mA$	5.5	6.2	7.5	V
V_{CLAMPL}	Input Low Clamp Voltage	$I_{DET}= -3mA$	0	0.65	1.00	V
$I_{ZCD,BS}$	Input Bias Current	$V_{ZCD}=1V \sim 5V$	-1.0	-0.1	1.0	μA
$I_{ZCD,SR}$	Source Current Capability ⁽⁴⁾	$T_A=25^{\circ}C$			-4	mA
$I_{ZCD,SK}$	Sink Current Capability ⁽⁴⁾	$T_A=25^{\circ}C$			10	mA
$t_{ZCD,D}$	Maximum Delay From ZCD to Output Turn-On ⁽⁴⁾	$dV/dt=-1V/100ns$, from 5V to 0V	100		200	ns
Output Section						
V_{OH}	Output Voltage High	$I_O=-100mA$, $T_A=25^{\circ}C$	9.2	11.0	12.8	V
V_{OL}	Output Voltage Low	$I_O=200mA$, $T_A=25^{\circ}C$		1.0	2.5	V
t_{RISE}	Rising Time ⁽⁴⁾	$C_{IN}=1nF$		50	100	ns
t_{FALL}	Falling Time ⁽⁴⁾	$C_{IN}=1nF$		50	100	ns
$V_{O,MAX}$	Maximum Output Voltage	$V_{CC}=20V$, $I_O=100\mu A$	11.5	13.0	14.5	V
$V_{O,UVLO}$	Output Voltage with UVLO Activated	$V_{CC}=5V$, $I_O=100\mu A$			1	V
Restart / Maximum Switching Frequency Limit Section						
t_{RST}	Restart Timer Delay		50	150	300	μs
f_{MAX}	Maximum Switching Frequency ⁽⁴⁾		250	300	350	kHz
Soft-Start Timer Section						
t_{SS}	Internal Soft-Soft ⁽⁴⁾		3	5	7	ms
Protections						
$V_{OVP,INV}$	OVP Threshold Voltage at INV pin	$T_A=25^{\circ}C$	2.620	2.675	2.730	V
$HY_{OVP,INV}$	OVP Hysteresis at INV pin	$T_A=25^{\circ}C$	0.120	0.175	0.230	V
$V_{OVP,OVP}$	OVP Threshold Voltage at OVP pin	$T_A=25^{\circ}C$	2.740	2.845	2.960	V
$HY_{OVP,OVP}$	OVP Hysteresis at OVP pin	$T_A=25^{\circ}C$		0.345		V
V_{EN}	Enable Threshold Voltage		0.40	0.45	0.50	V
HY_{EN}	Enable Hysteresis		0.05	0.10	0.15	V
T_{SD}	Thermal Shutdown Temperature ⁽⁴⁾		125	140	155	$^{\circ}C$
T_{HYS}	Hysteresis Temperature of TSD ⁽⁴⁾			60		$^{\circ}C$

Note:

4. These parameters, although guaranteed by design, are not production tested.

Comparison between FAN7530 and FAN7930B

Function	FAN7530	FAN7930B	FAN7930B Advantages
OVP Pin	None	Integrated	<ul style="list-style-type: none"> ▪ No External Circuit for additional OVP ▪ Reduction of Power Loss and BOM Cost Caused by additional OVP Circuit
Frequency Limit	None	Integrated	<ul style="list-style-type: none"> ▪ Abnormal CCM Operation Prohibited ▪ Abnormal Inductor Current Accumulation can be Prohibited
AC Absent Detection	None	Integrated	<ul style="list-style-type: none"> ▪ Increase System Reliability with AC On-Off Test ▪ Guarantee Stable Operation at Short Electric Power Failure
Soft-Start and Startup without Overshoot	None	Integrated	<ul style="list-style-type: none"> ▪ Reduce Voltage and Current Stress at Startup ▪ Eliminate Audible Noise due to Unwanted OVP Triggering
Control Range Compensation	None	Integrated	<ul style="list-style-type: none"> ▪ Can Avoid Burst Operation at Light Load and High Input Voltage ▪ Reduce Probability of Audible Noise Due to the Burst Operation
THD Optimizer	External	Internal	<ul style="list-style-type: none"> ▪ No External Resistor is Needed
TSD	None	140°C with 60°C Hysteresis	<ul style="list-style-type: none"> ▪ Stable and Reliable TSD Operation ▪ Converter Temperature Range Limited Range

Comparison between FAN7930 and FAN7930B

Function	FAN7930	FAN7930B	FAN7930B Remark
RDY Pin	Integrated	None	<ul style="list-style-type: none"> ▪ User Choice for the Use of Number #2 Pin
OVP Pin	None	Integrated	
Control Range Compensation	None	Integrated	

Typical Performance Characteristics

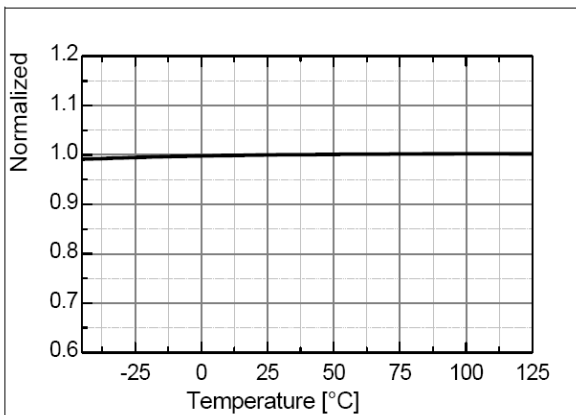


Figure 4. Voltage Feedback Input Threshold 1 (V_{REF1}) vs. T_A

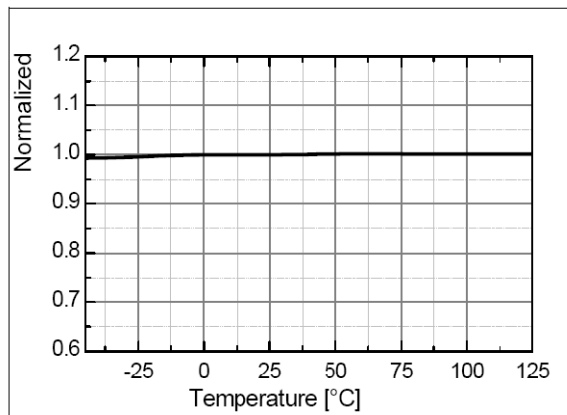


Figure 5. Start Threshold Voltage (V_{START}) vs. T_A

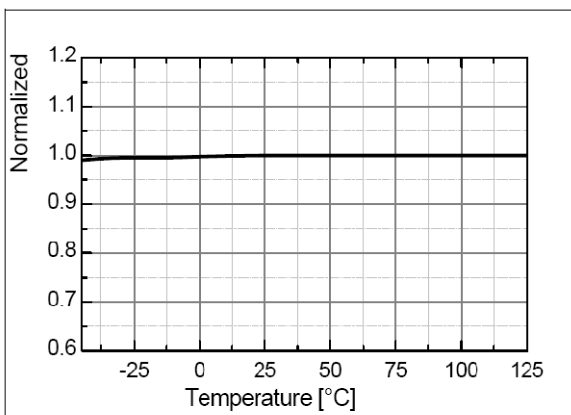


Figure 6. Stop Threshold Voltage (V_{STOP}) vs. T_A

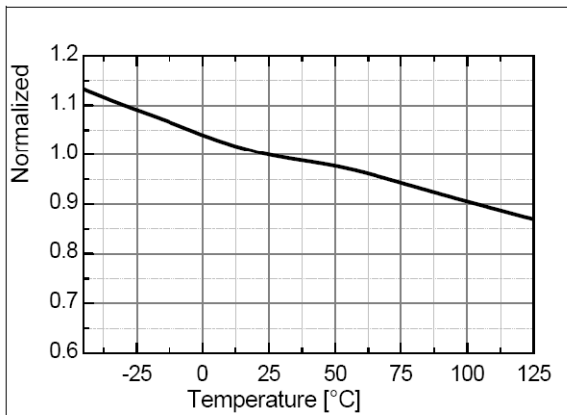


Figure 7. Startup Supply Current (I_{START}) vs. T_A

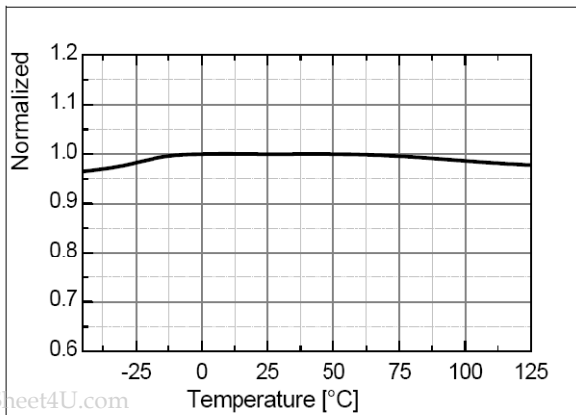


Figure 8. Operating Supply Current (I_{OP}) vs. T_A

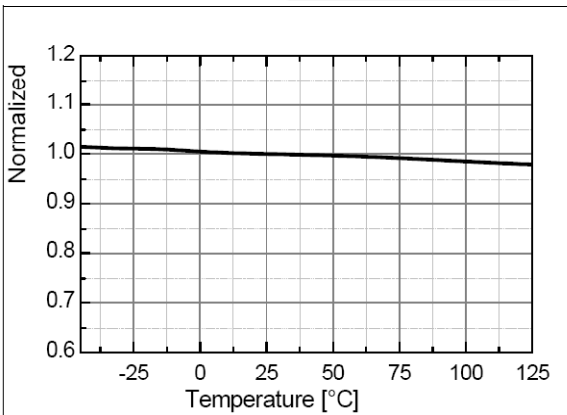


Figure 9. Output Upper Clamp Voltage (V_{EAH}) vs. T_A

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Typical Performance Characteristics

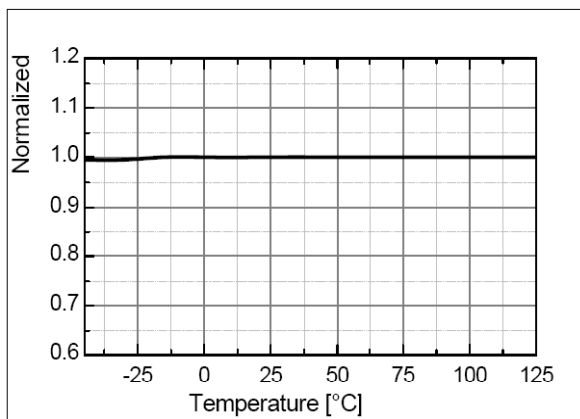


Figure 10. Zero Duty Cycle Output Voltage (V_{Eaz}) vs. T_A

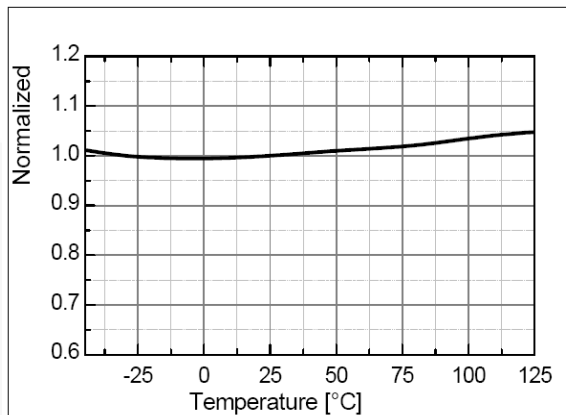


Figure 11. Maximum On-Time Program 1 ($t_{ON,MAX1}$) vs. T_A

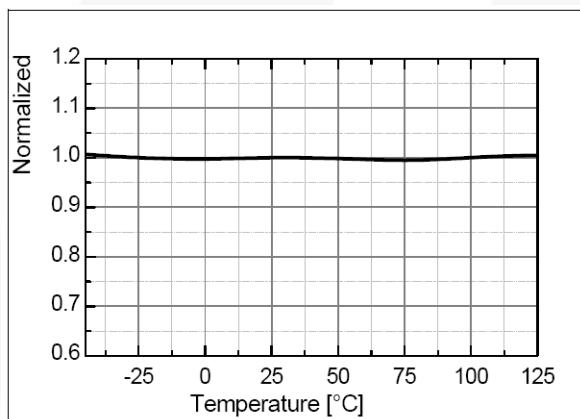


Figure 12. Maximum On-Time Program 2 ($t_{ON,MAX2}$) vs. T_A

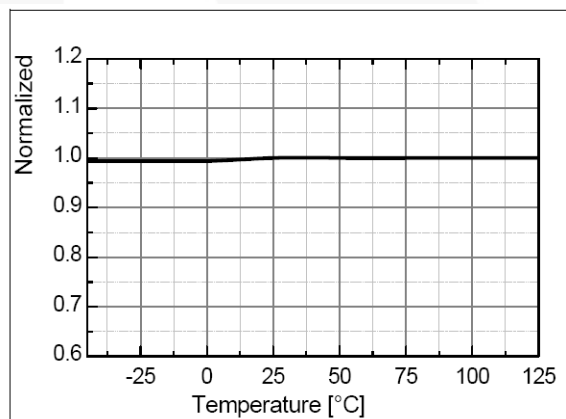


Figure 13. Current Sense Input Threshold Voltage Limit (V_{CS}) vs. T_A

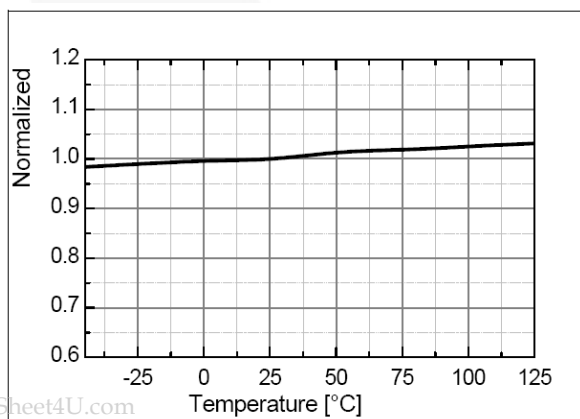


Figure 14. Input High Clamp Voltage (V_{CLAMPH}) vs. T_A

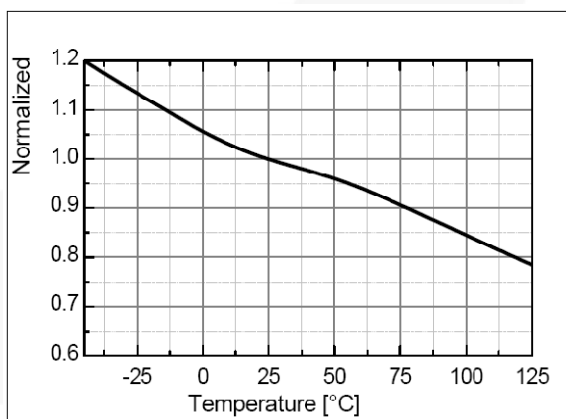


Figure 15. Input Low Clamp Voltage (V_{CLAMPL}) vs. T_A

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Typical Performance Characteristics

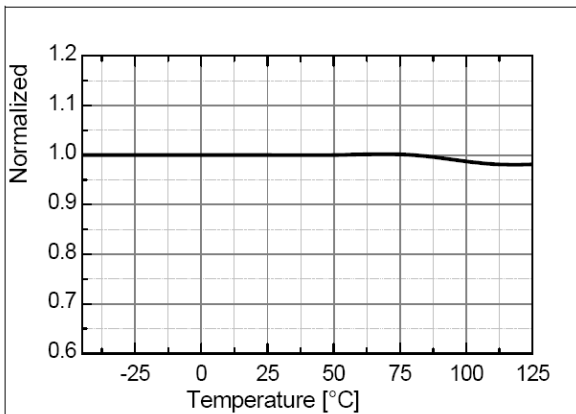


Figure 16. Output Voltage High (V_{OH}) vs. T_A

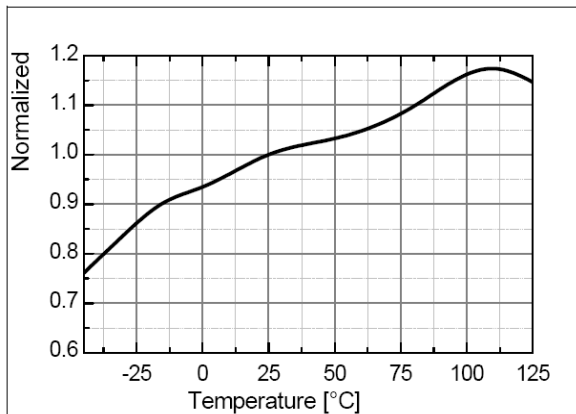


Figure 17. Output Voltage Low (V_{OL}) vs. T_A

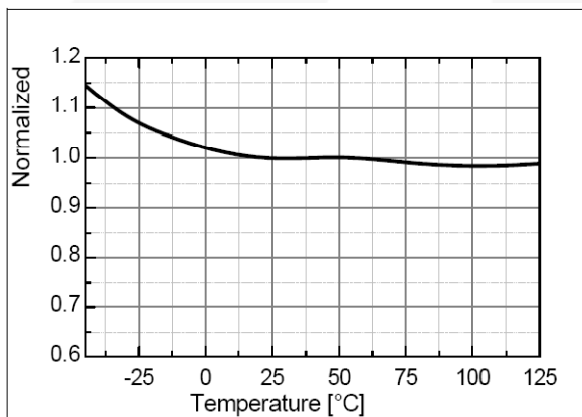


Figure 18. Restart Timer Delay (t_{RST}) vs. T_A

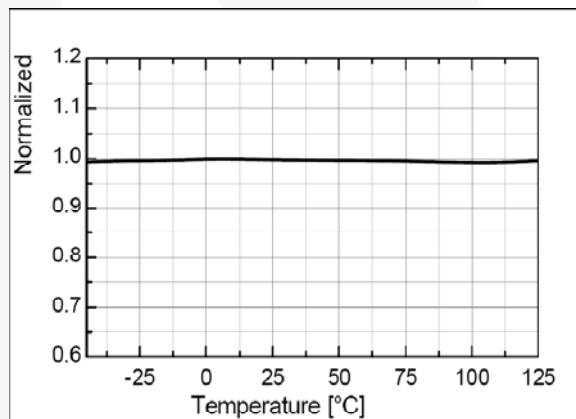


Figure 19. OVP Threshold at OVP Pin (V_{OVP,OVP}) vs. T_A

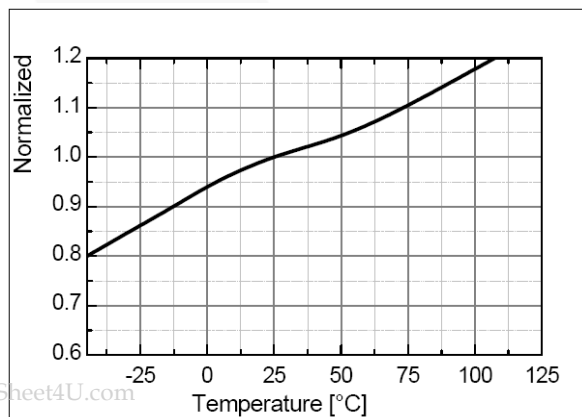


Figure 20. Output Saturation Voltage (V_{RDY,SAT}) vs. T_A

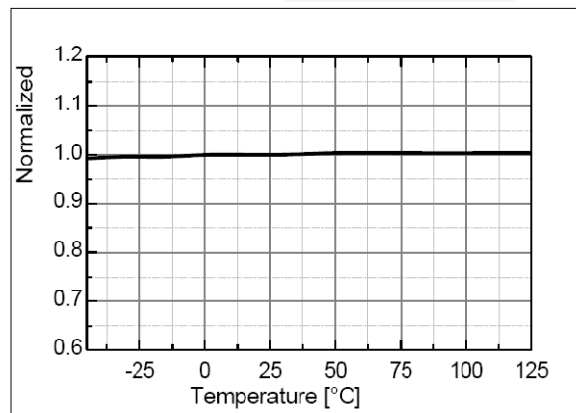


Figure 21. OVP Threshold Voltage (V_{OVP}) vs. T_A

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Applications Information

1. Startup: Normally, supply voltage (V_{CC}) of a PFC block is fed from the additional power supply, which can be called standby power. Without this standby power, auxiliary winding to detect zero current detection can be used as a supply source. Once the supply voltage of the PFC block exceeds 12V, internal operation is enabled until the voltage drops to 8.5V. If V_{CC} exceeds V_Z , 20mA current is sinking from V_{CC} .

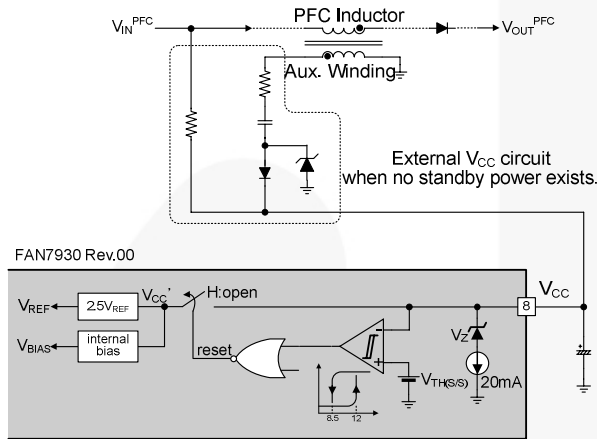


Figure 22. Startup Circuit

2. INV Block: Scaled-down voltage from the output is the input for the INV pin. Many functions are embedded based on the INV pin: transconductance amplifier, output OVP comparator and disable comparator.

For the output voltage control, a transconductance amplifier is used instead of the conventional voltage amplifier. The transconductance amplifier (voltage-controlled current source) aids the implementation of OVP and disables function. The output current of the amplifier changes according to the voltage difference of the inverting and non-inverting input of the amplifier. To cancel down the line input voltage effect on power factor correction, effective control response of PFC block should be slower than the line frequency and these conflicts with the transient response of controller. Two-pole one-zero type compensation may be used to meet both requirements.

The OVP comparator shuts down the output drive block when the voltage of the INV pin is higher than 2.675V and there is 0.175V hysteresis. The disable comparator disables the operation when the voltage of the inverting input is lower than 0.35V and there is 100mV hysteresis. An external small-signal MOSFET can be used to disable the IC. The IC operating current decreases to reduce power consumption if the IC is disabled. 0 is the timing chart of the internal circuit near the INV pin when rated PFC output voltage is assumed at 390V_{DC} and V_{CC} supply voltage is 15V.

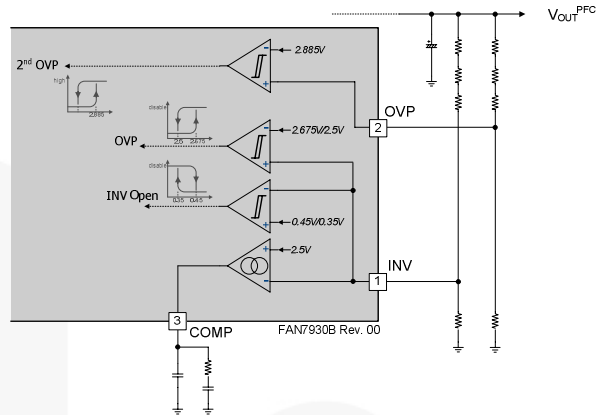


Figure 23. Circuit Around INV Pin

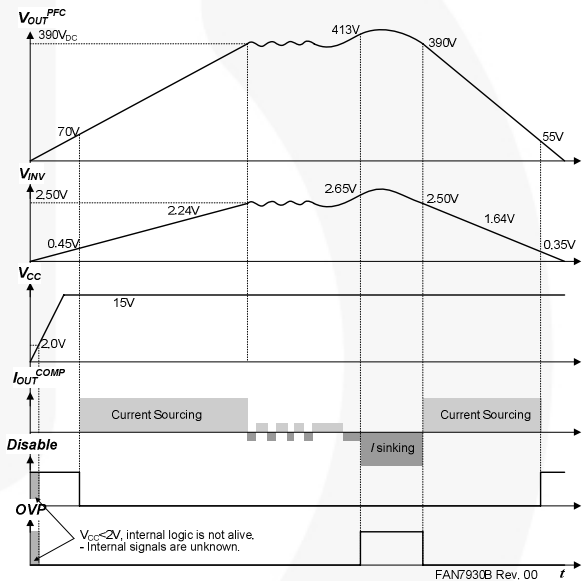


Figure 24. Timing Chart for INV Block

3. OVP Pin: Over-Voltage Protection (OVP) is embedded by the information at the INV pin. That information comes from the output through the voltage dividing resistors. To scale down from high voltage to low one, high resistance normally used with low resistance. In cases the resistor of high resistance get a damage and resistance is changed to high, though INV pin information is normal output voltage exceeds its rated output. Once this happen, output electrolytic capacitor may be exploded. To prevent such a catastrophe additional OVP pin is assigned to double check output voltage. Thus additional OVP may be called 2nd OVP while INV pin OVP can be called 1st OVP.

Since the two OVP conditions are quite different, protection recovering mode is different. Once the first OVP triggers, switching stops immediately and recovers switching when the output voltage is decreased with a hysteresis. When the second OVP triggers, switching can be recovered only when the V_{CC} supply voltage falls below V_{STOP} and builds up higher than V_{START} again and V_{OVP} should be lower than hysteresis. If the second OVP is not used, the OVP pin must be connected to the INV pin or to the ground.

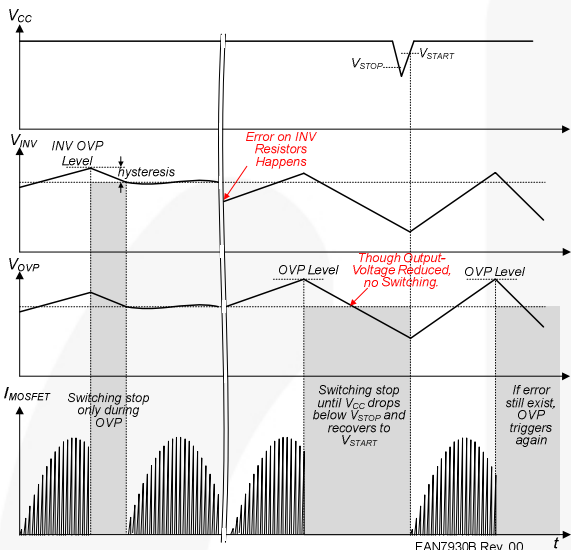


Figure 25. Comparison of 1st and 2nd OVP Recovering Mode

4. Control Range Compensation: On time is controlled by the output voltage compensator with FAN7930B. Due to this when input voltage is high and load is light, control range become narrow compared when input voltage is low. That control range decrease is anti-proportional to the double square of the input voltage. Thus at high line unwanted burst operation easily happens at light load and audible noise may be generated from the boost inductor or inductor at input filter. Different from the other converters, burst operation in PFC block is not needed because PFC block itself is normally disabled during standby mode. To improve this kind of unwanted burst operation at light load, internal control range compensation function is implemented and approximately shows no burst operation until 5% load at high line.

5. Zero-Current Detection: Zero-current detection (ZCD) generates the turn-on signal of the MOSFET when the boost inductor current reaches zero using an auxiliary winding coupled with the inductor. When the power switch turns on, negative voltage is induced at the auxiliary winding due to the opposite winding direction (see Equation 1) and positive voltage is induced (see Equation 2) when the power switch turns off.

$$V_{AUX} = -\frac{T_{AUX}}{T_{IND}} \cdot V_{AC} \quad (1)$$

$$V_{AUX} = \frac{T_{AUX}}{T_{IND}} \cdot (V_{PFCOUT} - V_{AC}) \quad (2)$$

where, V_{AUX} is the auxiliary winding voltage, T_{IND} and T_{AUX} are boost inductor turns and auxiliary winding turns respectively, V_{AC} is input voltage for PFC converter and V_{OUT_PFC} is output voltage from the PFC converter.

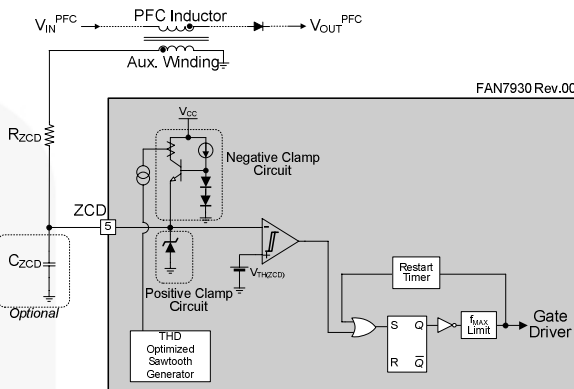


Figure 26. Circuit Near ZCD

Because auxiliary winding voltage can swing from negative voltage to positive voltage, the internal block in ZCD pin has both positive and negative voltage clamping circuits. When the auxiliary voltage is negative, internal circuit clamps the negative voltage at the ZCD pin around 0.65V by sourcing current to the serial resistor between the ZCD pin and the auxiliary winding. When the auxiliary voltage is higher than 6.5V, current is sunk through a resistor from the auxiliary winding to the ZCD pin.

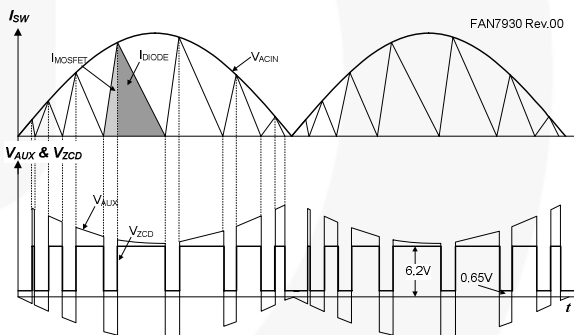


Figure 27. Auxiliary Voltage Depends on MOSFET Switching

To check the boost inductor current zero instance, auxiliary winding voltage is used. When boost inductor current becomes zero, there is a resonance between boost inductor and all capacitors at MOSFET drain pin, including C_{OSS} of the MOSFET; an external capacitor at the D-S pin to reduce the voltage rising and falling slope of the MOSFET; a parasitic capacitor at inductor; and so on to improve performance. Resonated voltage is reflected to the auxiliary winding and can be used as detecting zero current of boost inductor and valley position of MOSFET voltage stress. For valley detection, a minor delay by the resistor and capacitor is needed. A capacitor increases the noise immunity at the ZCD pin. If ZCD voltage is higher than 1.5V, an internal ZCD comparator output becomes HIGH and LOW when the ZCD goes below 1.4V. At the falling edge of comparator output, internal logic turns on the MOSFET.

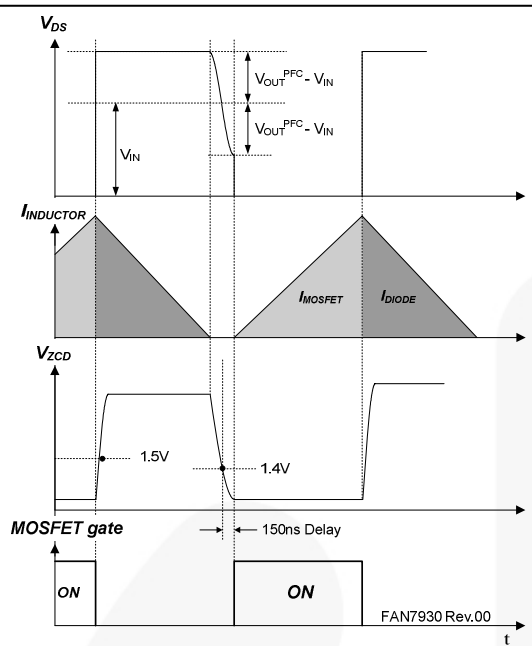


Figure 28. Auxiliary Voltage Threshold

When no ZCD signal is available, the PFC controller cannot turn on MOSFET, so the controller checks every switching off time and forces MOSFET turn on when the off time is longer than 150 μ s. It is called restart timer. Restart timer triggers MOSFET turn on at startup and may be used at the input voltage zero cross period.

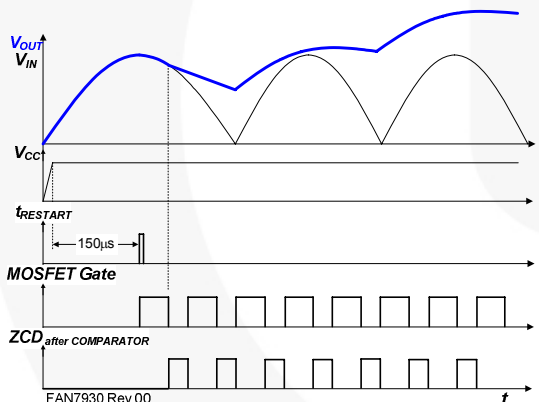


Figure 29. Restart Timer at Startup

Because the MOSFET turn on depends on the ZCD input, switching frequency may increase to higher than several megahertz due to the miss-triggering or noise on the nearby ZCD pin. If the switching frequency is higher than needed for critical conduction mode (CRM), operation mode shifts to continuous conduction mode (CCM). In CCM, unlike CRM where the boost inductor current is reset to zero at the next switch on; inductor current builds up at every switching cycle and can be raised to very high current, that exceeds the current rating of the power switch or diode. This can seriously damage the power switch and result in burn down. To avoid this, maximum switching frequency limitation is embedded. If ZCD signal is applied again within 3.3 μ s after the previous rising edge of gate signal, this signal is ignored internally and FAN7930B waits for another ZCD signal. This slightly degrades the power factor performance at light load and high input voltage.

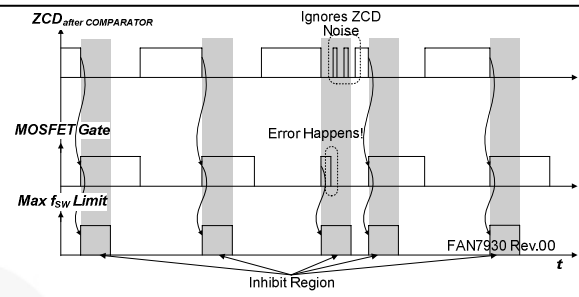


Figure 30. Maximum Switching Frequency Limit Operation

6. Control: The scaled output is compared with the internal reference voltage and sinking or sourcing current is generated from the COMP pin by the transconductance amplifier. The error amplifier output is compared with the internal sawtooth waveform to give proper turn-on time based on the controller.

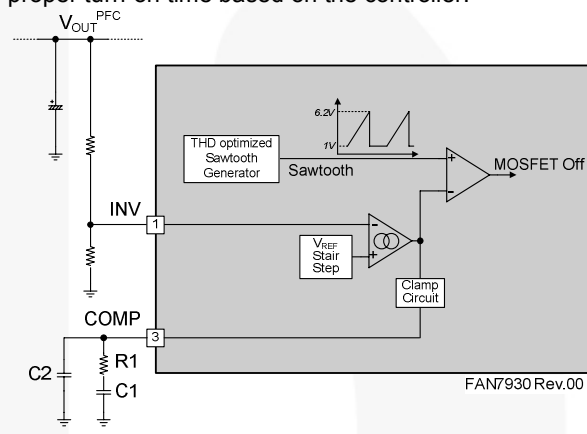


Figure 31. Control Circuit

Unlike a conventional voltage-mode PWM controller, FAN7930B turns on the MOSFET at the falling edge of ZCD signal. On instance is decided by the external signal and the turn-on time lasts until the error amplifier output (V_{COMP}) and sawtooth waveform meet. When load is heavy, output voltage decreases, scaled output decreases, COMP voltage increases to compensate low output, turn-on time lengthens to give more inductor turn-on time, and increased inductor current raises the output voltage. This is how PFC negative feedback controller regulates output.

The maximum of V_{COMP} is limited to 6.5V, which dictates the maximum turn-on time, and switching stops when V_{COMP} is lower than 1.0V.

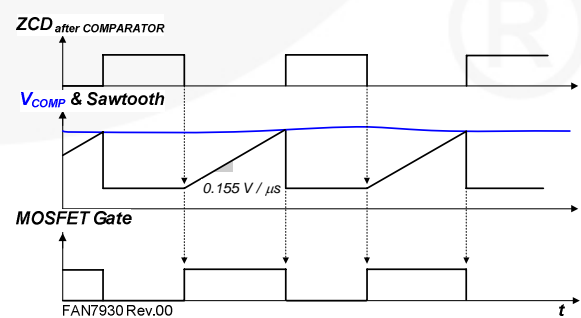


Figure 32. Turn-On Time Determination

The roles of PFC controller are regulating output voltage and input current shaping to increase power factor. Duty control based on the output voltage should be fast enough to compensate output voltage dip or overshoot. For the power factor, however, the control loop must not react to the fluctuating AC input voltage. These two requirements conflict; therefore, when designing a feedback loop, the feedback loop should be least 10 times slower than AC line frequency. That slow response is made by C1 at compensator. R1 makes gain boost around operation region and C2 attenuates gain at higher frequency. Boost gain by R1 helps raise the response time and improves phase margin.

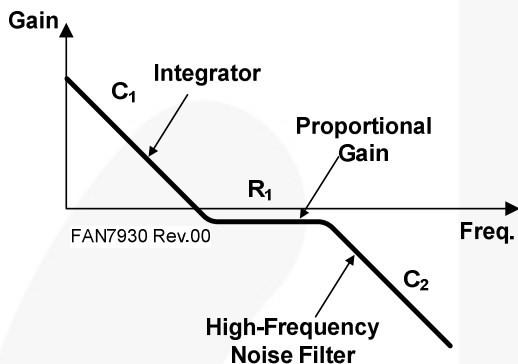


Figure 33. Compensators Gain Curve

For the transconductance error amplifier side, gain changes based on differential input. When the error is large, gain is large to make the output dip or peak to suppress quickly. When the error is small, low gain is used to improve power factor performance.

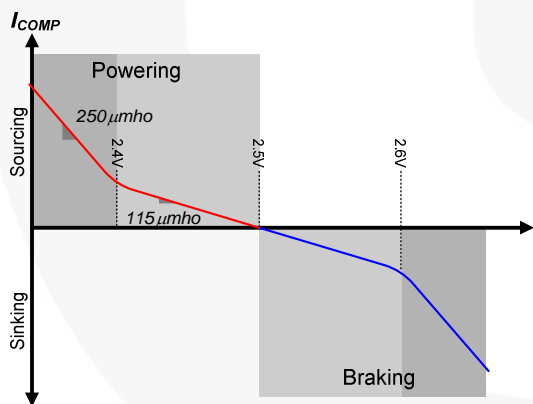


Figure 34. Gain Characteristic

7. Soft-Start: When V_{CC} touches V_{START} , internal reference voltage is increased like a stair step for 5ms. As a result, V_{COMP} is also raised gradually and MOSFET turn-on time increases smoothly. This reduces voltage and current stress on the power switch during startup.

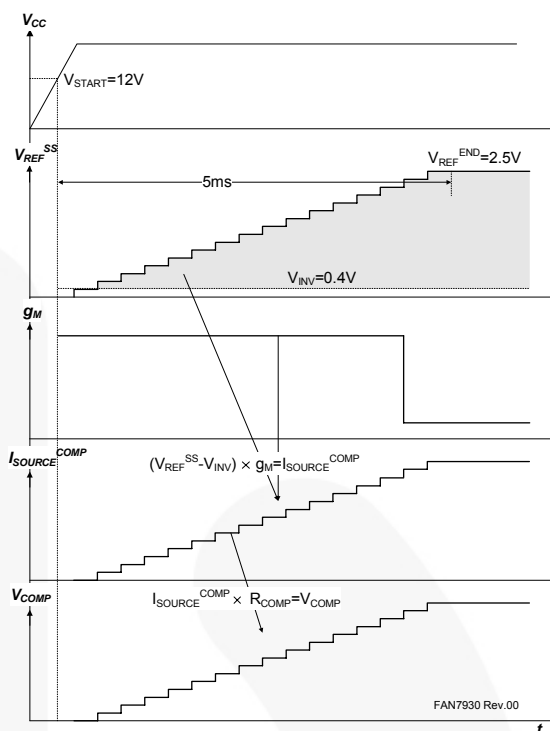


Figure 35. Soft-Start Sequence

8. Startup without Overshoot: Feedback control speed of PFC is quite slow. Due to the slow response, there is a gap between output voltage and feedback control. That is why over-voltage protection (OVP) is critical at the PFC controller and voltage dip caused by fast load changes from light to heavy is diminished by a bulk capacitor. OVP is easily triggered at startup phase. Operation on and off by OVP at startup may cause audible noise and can increase voltage stress at startup, which is normally higher than in normal operation. This operation is better when soft-start time is very long. However, too long startup time enlarges the output voltage building time at light load. FAN7930B has “overshoot-less” control at startup. During startup, the feedback loop is controlled by an internal proportional gain controller and when the output voltage reaches the rated value, it switches to an external compensator after a transition time of 30ms. In short, an internal proportional gain controller eliminates overshoot at startup and an external conventional compensator takes over successfully afterward.

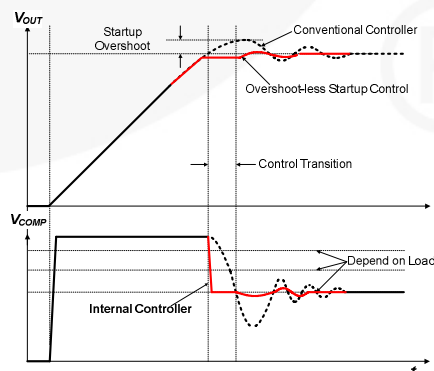


Figure 36. Overshoot-less Startup Control

9. THD Optimization: Total harmonic distortion (THD) is the factor that dictates how closely input current shape matches sinusoidal form. The turn-on time of the PFC controller is almost constant over one AC line period due to the extremely low feedback control response. The turn-off time is decided by the current decrease slope of the boost inductor made by the input voltage and output voltage. Once inductor current becomes zero, resonance between C_{OSS} and the boost inductor makes oscillating waveforms at the drain pin and auxiliary winding. By checking the auxiliary winding voltage through the ZCD pin, the controller can check the zero current of boost inductor. At the same time, a minor delay time is inserted to determine the valley position of drain voltage. The input and output voltage difference is at its maximum at the zero cross point of AC input voltage. The current decrease slope is steep near the zero cross region and more negative inductor current flows during a drain voltage valley detection time. Such a negative inductor current cancels down the positive current flows and input current becomes zero, called “zero-cross distortion” in PFC.

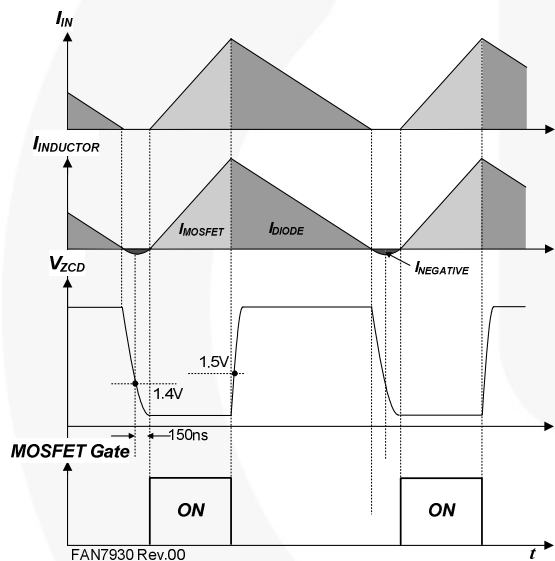


Figure 37. Input and Output Current Near Input Voltage Peak

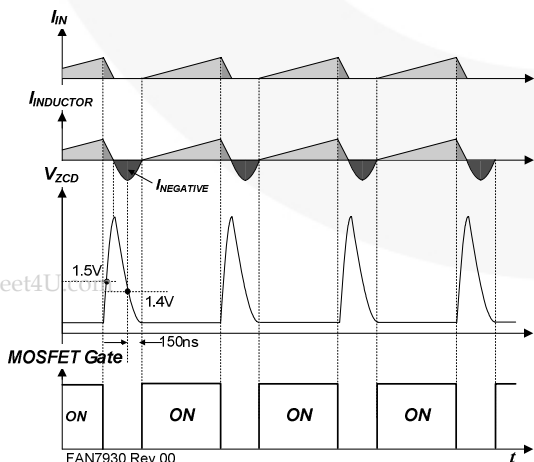


Figure 38. Input and Output Current Near Input Voltage Peak Zero Cross

To improve this, lengthened turn-on time near the zero cross region is a well-known technique, though the method may be different from company to company and may be proprietary. FAN7930B embodies this by sourcing current through the ZCD pin. Auxiliary winding voltage becomes negative when the MOSFET turns on and is proportional to input voltage. The negative clamping circuit of ZCD outputs the current to maintain the ZCD voltage at a fixed value. The sourcing current from the ZCD is directly proportional to the input voltage. Some portion of this current is applied to the internal sawtooth generator together with a fixed-current source. Theoretically, the fixed-current source and the capacitor at sawtooth generator decide the maximum turn-on time when no current is sourcing at ZCD clamp circuit and available turn-on time gets shorter proportional to the ZCD sourcing current.

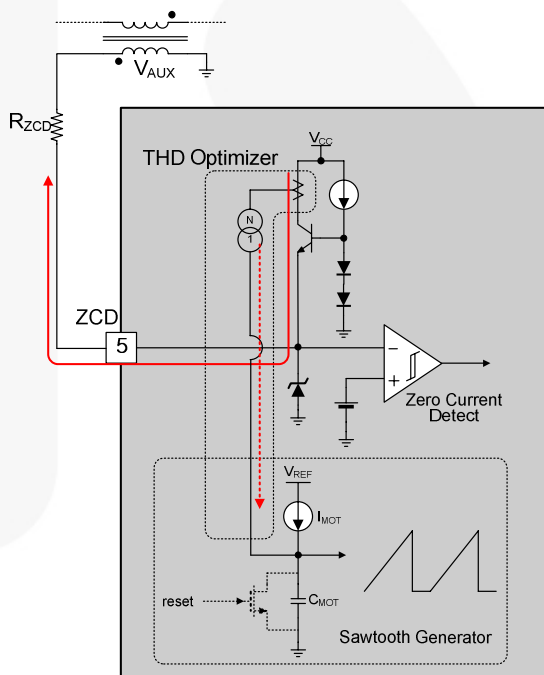


Figure 39. Circuit of THD Optimizer

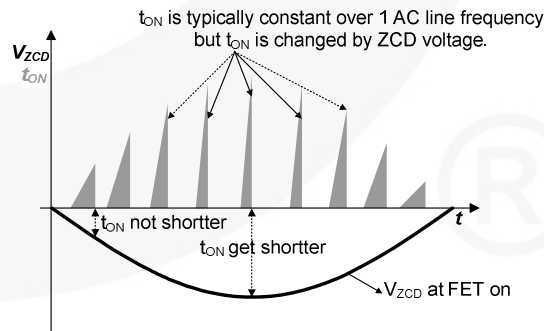


Figure 40. Effect of THD Optimizer

By THD optimizer, turn-on time over one AC line period is proportionally changed, depending on input voltage. Near zero cross, lengthened turn-on time improves THD performance.

10. Input Voltage Absent Detection: To save power loss caused by input voltage sensing resistors and to optimize THD easily, the FAN7930B omits AC input voltage detection. Therefore, no information about AC input is available from the internal controller. In many cases, the V_{CC} of PFC controller is supplied by an independent power source like standby power. In this scheme, some mismatch may exist. For example, when the electric power is suddenly interrupted during two or three AC line periods; V_{CC} is still alive during that time, but output voltage drops because there is no input power source. Consequently, the control loop tries to compensate for the output voltage drop and V_{COMP} reaches its maximum. This lasts until AC input voltage is live again. When AC input voltage is live again, high V_{COMP} allows high switching current and more stress is put on the MOSFET and diode. To protect against this, FAN7930B internally checks if the input AC voltage exists. If input does not exist, soft-start is reset and waits until AC input is live again. Soft-start manages the turn-on time for smooth operation when it detects AC input is applied again and applies less voltage and current stress on startup.

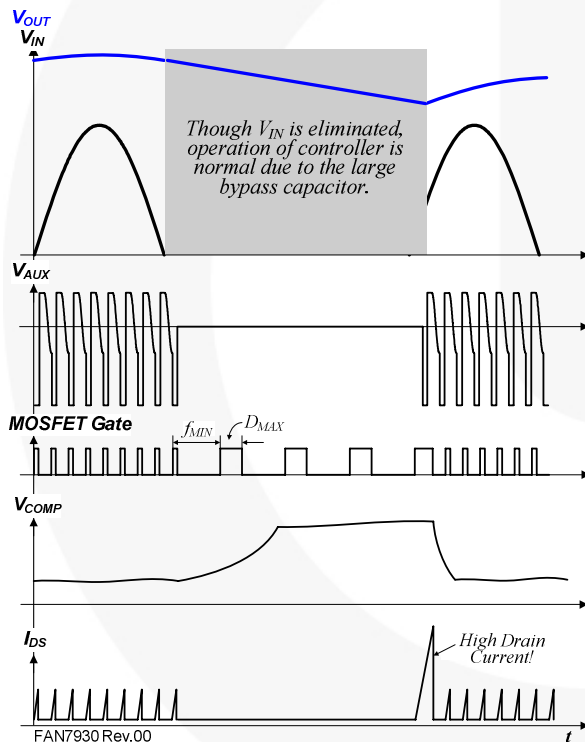


Figure 41. Operation without Input Voltage Absent Circuit

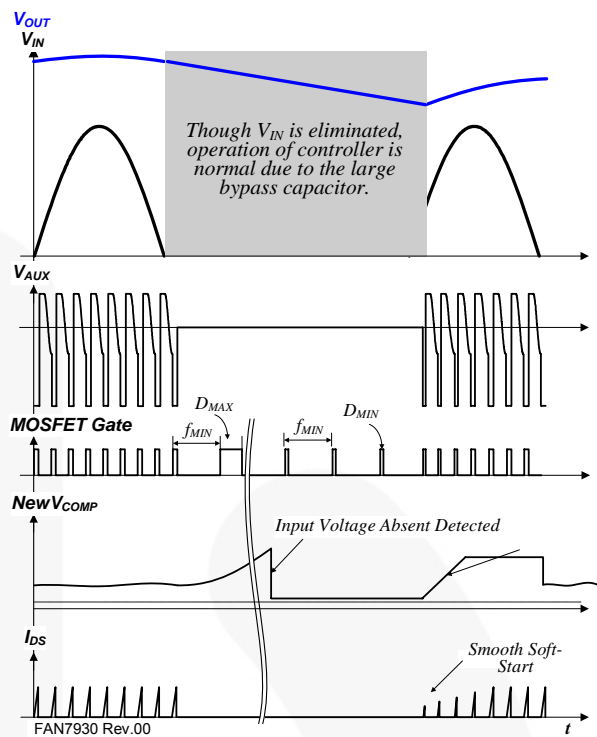


Figure 42. Operation with Input Voltage Absent Circuit

11. Current Sense: The MOSFET current is sensed using an external sensing resistor for the over-current protection. If the CS pin voltage is higher than 0.8V, the over-current protection comparator generates a protection signal. An internal RC filter of 40k Ω and 8pF is included to filter switching noise.

12. Gate Driver Output: FAN7930B contains a single totem-pole output stage designed for a direct drive of the power MOSFET. The drive output is capable of up to +500/-800mA peak current with a typical rise and fall time of 50ns with 1nF load. The output voltage is clamped to 13V to protect the MOSFET gate even if the V_{CC} voltage is higher than 13V.

PCB Layout Guide

PFC block normally handles high switching current and the voltage low energy signal path can be affected by the high energy path. Cautious PCB layout is mandatory for stable operation.

1. The gate drive path should be as short as possible. The closed-loop that starts from the gate driver, MOSFET gate, and MOSFET source to ground of PFC controller is recommended as close as possible. This is also crossing point between power ground and signal ground. Power ground path from the bridge diode to the output bulk capacitor should be short and wide. The sharing position between power ground and signal ground should be only at one position to avoid ground loop noise. Signal path of PFC controller should be short and wide for external components to contact.
2. PFC output voltage sensing resistor is normally high to reduce current consumption. This path can be affected by external noise. To reduce noise possibility at the INV pin, a shorter path for output sensing is recommended. If a shorter path is not possible, place some dividing resistors between PFC output and the INV pin — closer to the INV pin is better. Relative high voltage close to the INV pin can be helpful.
3. ZCD path is recommended close to auxiliary winding from boost inductor and to the ZCD pin. If that is difficult, place a small capacitor (below 50pF) to reduce noise.
4. Switching current sense path should not share with another path to avoid interference. Some additional components may be needed to reduce the noise level applied to the CS pin.

5. A stabilizing capacitor for V_{CC} is recommended as close as possible to the V_{CC} and ground pins. If it is difficult, place the SMD capacitor as close to the corresponding pins as possible.

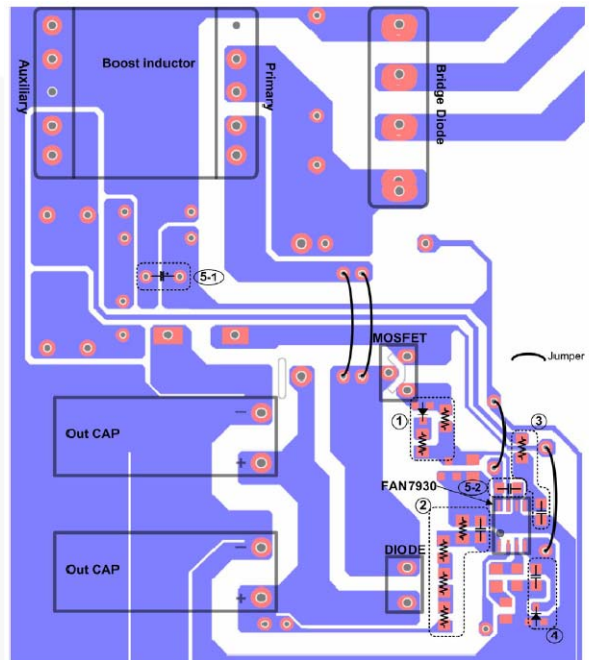


Figure 43. Recommended PCB Layout

2. Transformer

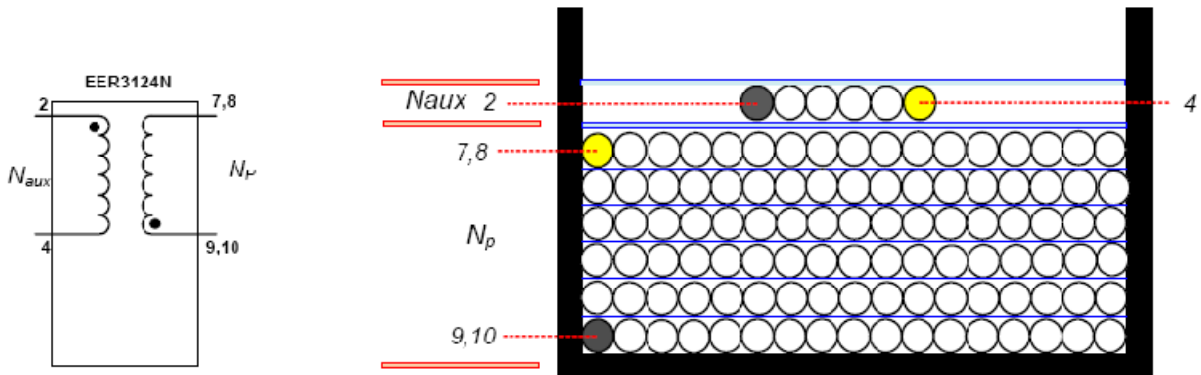


Figure 45. Transformer Schematic Diagram of FAN7930B

3. Winding Specification

Position	No	Pin (S → F)	Wire	Turns	Winding Method	Barrier Tape		
						TOP	BOT	Ts
Bottom	N _p	9, 10 → 7, 8	0.1φ×50	49	Solenoid Winding			1
	Insulation: Polyester Tape t = 0.025mm, 3 Layers							
Top	N _{AUX}	2 → 4	0.3φ	6	Solenoid Winding			
	Insulation: Polyester Tape t = 0.025mm, 4 Layers							

4. Electrical Characteristics

	Pin	Specification	Remark
Inductance	9, 10 → 7, 8	230μH ± 7%	100kHz, 1V

5. Core & Bobbin

Core: EER3124, Samhwa (PL-7) (Ae=97.9mm²)

Bobbin: EER3124

6. Bill of Materials

Part #	Value	Note	Part #	Value	Note
Resister			Switch		
R101	1M Ω	1W	Q101	FCPF20N60	20A, 600V, SuperFET
R102	330 k Ω	1/2W	Diode		
R103	10 k Ω	1W	D101	1N4746	1W, 18V, Zener Diode
R104	30k Ω	1/4W	D102	UF4004	1A, 400V Glass Passivated High-Efficiency Rectifier
R107	10k Ω	1/4W	D103	1N4148	1A, 100V Small-Signal Diode
R108	4.7k Ω	1/4W	D104	1N4148	1A, 100V Small-Signal Diode
R109	47k Ω	1/4W	D105		8A, 600V, General-Purpose Rectifier
R110	10k Ω	1/4W	D106		3A, 600V, General-Purpose Rectifier
R111	0.80k Ω	5W			
R112, 113, 114,116,117,118	3.9k Ω	1/4W	IC101	FAN7930B	CRM PFC Controller
R115,119	75k Ω	1/4W			
Capacitor			Fuse		
C101	220nF/275V _{AC}	Box Capacitor	FS101	5A/250V	
C102	680nF/275V _{AC}	Box Capacitor	NTC		
C103	0.68 μ F/630V	Box Capacitor	TH101	5D-15	
C104	12nF/50V	Ceramic Capacitor	Bridge Diode		
C105	100nF/50V	SMD (1206)	BD101		15A, 600V
C107	33 μ F/50V	Electrolytic Capacitor	Line Filter		
C108	220nF/50V	Ceramic Capacitor	LF101	23mH	
C109	47nF/50V	Ceramic Capacitor	Transformer		
C110,116	1nF/50V	Ceramic Capacitor	T1	EER3124	Ae=97.9mm ²
C112	47nF/50V	Ceramic Capacitor	ZNR		
C111	220 μ F/450V	Electrolytic Capacitor	ZNR101	10D471	
C114	2.2nF/450V	Box Capacitor			
C115	2.2nF/450V	Box Capacitor			

Physical Dimensions

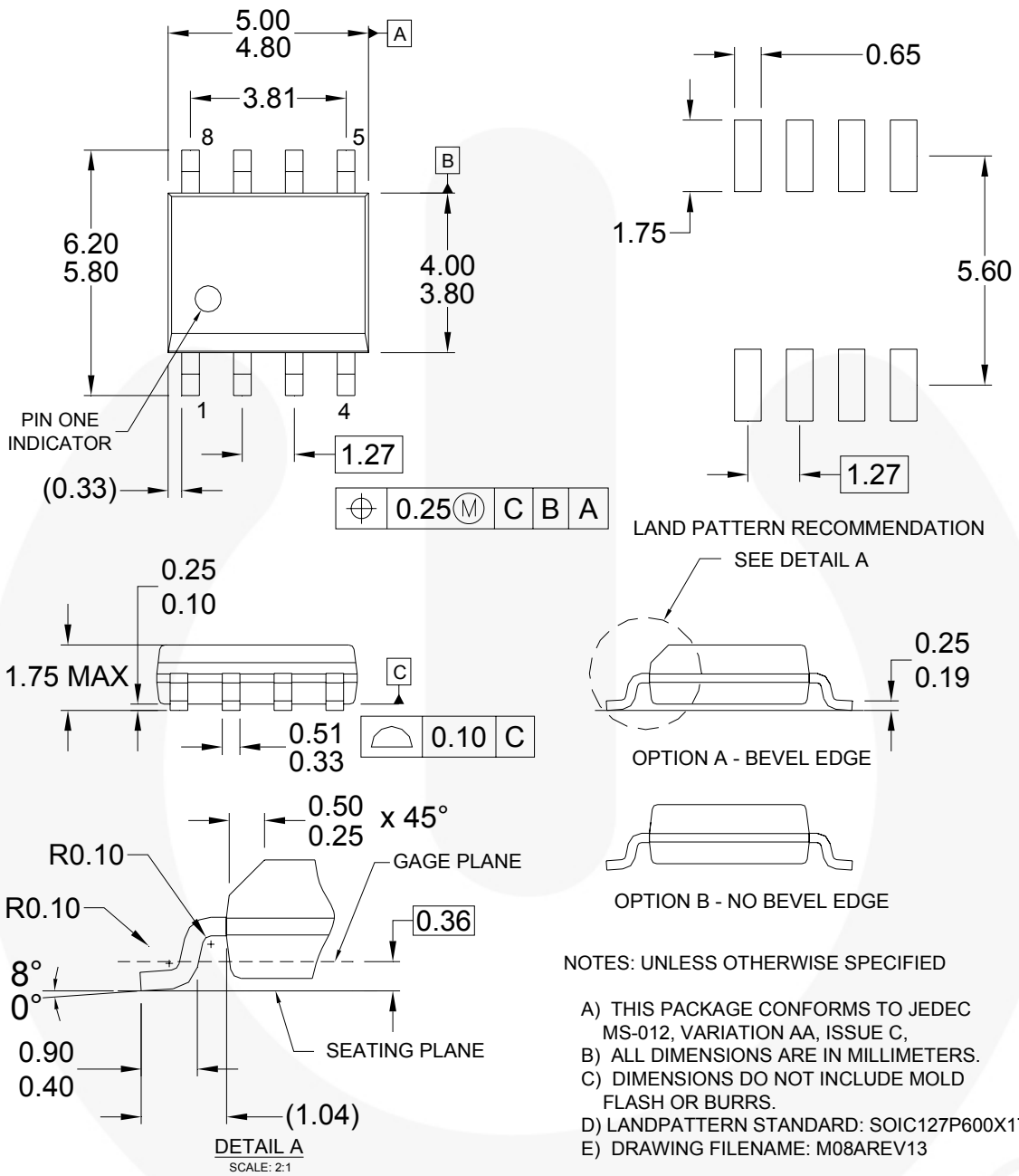


Figure 46. 8-Lead Small Outline Package (SOP)

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